1MHz, 2A, High-Efficiency PWM Synchronous Step-Down Converter

Description

The FP6361 is a high efficiency, low-noise, DC-DC step-down pulse width modulated (PWM) converter. The 100% duty cycle feature provides low dropout operation, extending battery life in portable systems. Switch frequency is internally set at 1MHz, which allows use of small surface mount inductors and capacitors.

The internal synchronous switch increases efficiency and eliminates the need for an external Schottky diode. Shutdown mode places the device in standby, reducing quiescent supply current to less than 1µA.

The current limit protection and on-chip thermal shutdown features provide protection against any combination of overload or ambient temperature.

Features

- Synchronous Rectification: Approach 95% Efficiency
- 2.6V to 5.5V Input Voltage Range
- Real Shutdown Isolated Load from Battery
- Internal Compensation without External Capacitors and Resistors
- No Schottky Diode Required
- Low Dropout Operation: 100% Duty Cycle
- Fixed Frequency Operation at 1MHz
- Very Low Shutdown Current Less than 1µA
- Over Temperature Protection
- RoHS Compliant

Applications

- Cellular Phone
- Handheld Instrument
- Wireless LAN
- Microprocessors and DSP
- Battery Operated Device

Pin Assignments

WQ Package TQFN-16 (3mmx3mm)

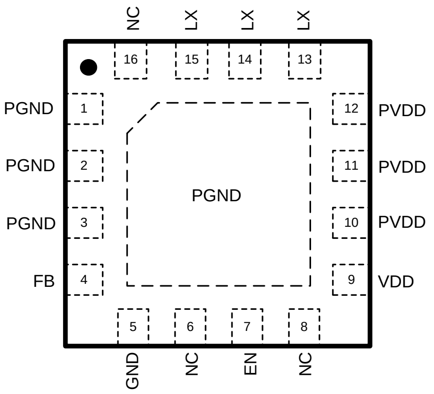
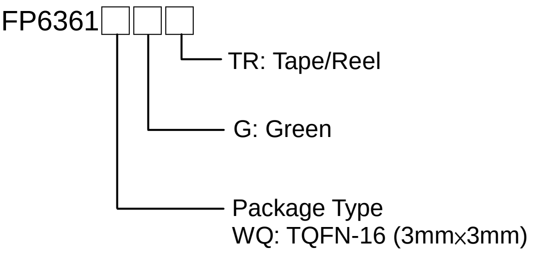


Figure1. Pin Assignment of FP6361

Ordering Information



Typical Application Circuit

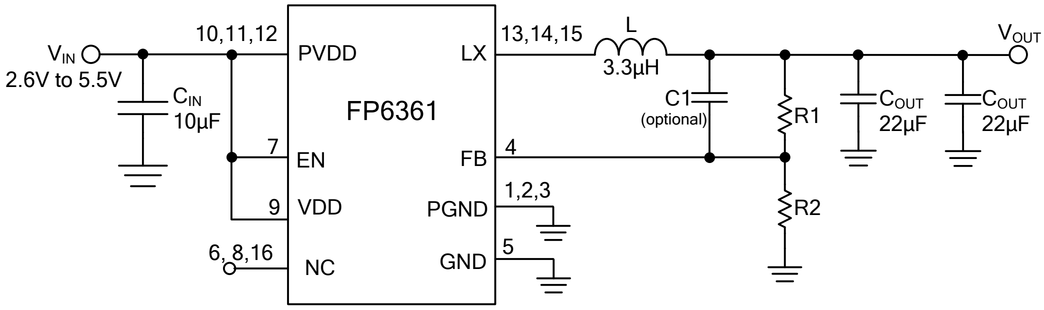


Figure 2. Typical application circuit

Functional Pin Description

Pin Name	Pin Function
PGND	Power Ground.
FB	Feedback Input.
NC	No Connection.
GND	Signal Ground.
EN	Enable Pin. Logic high enables the converter, and logic low forces the device into shutdown mode to reduce the supply current to less than 1µA.
VDD	Supply Voltage Input. Input range is from 2.6V to 5.5V.
PVDD	Supply Voltage Input. Input range is from 2.6V to 5.5V.
LX	Inductor connection to the drains of the internal power MOSFETs.

Block Diagram

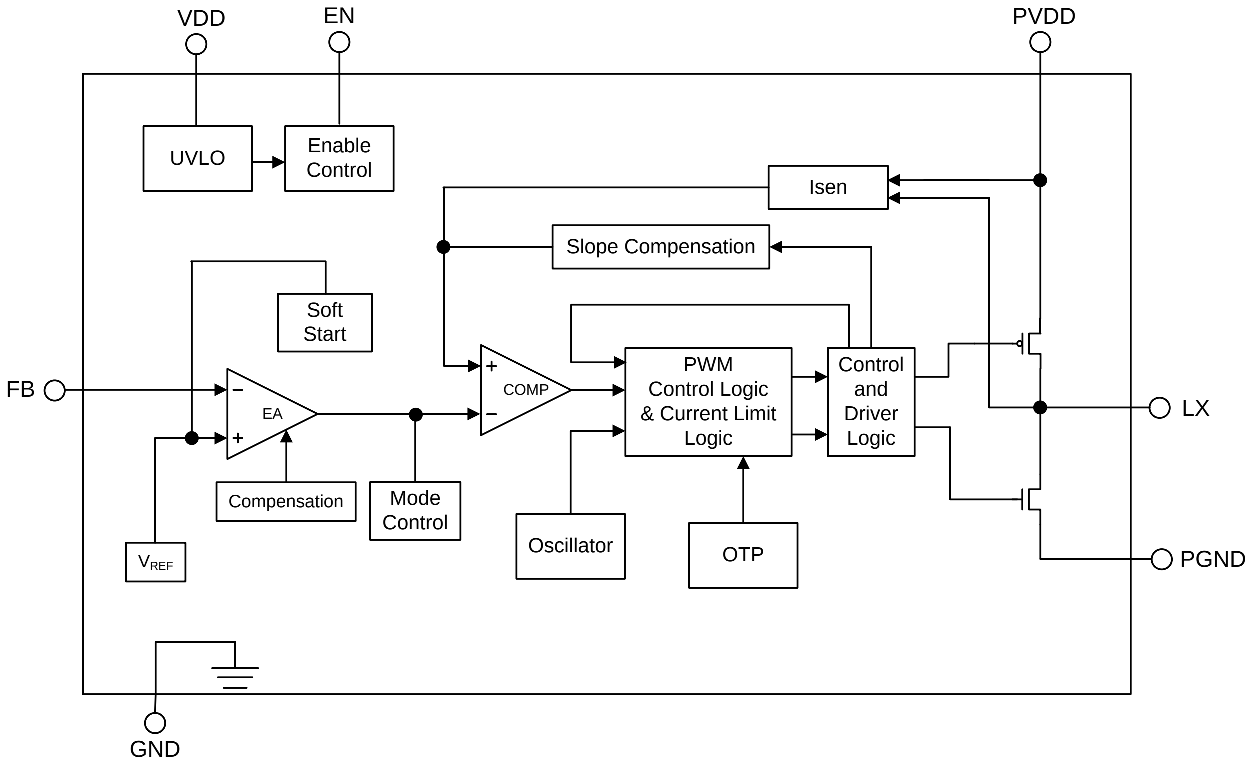


Figure 3. Block Diagram of FP6361

Absolute Maximum Ratings

- VDD, PVDD to GND -- -0.3V to +6V
- LX to GND --- -0.3V to (V_{DD}+0.3)
- EN, FB to GND -- -0.3V to V_{DD}
- Power Dissipation @25°C: TQFN-16 (3mm×3mm) (P_D) --- +1.54W
- Package Thermal Resistance TQFN-16 (3mm×3mm) (θ_{JA}) ------------------------------------- +65°C/W
- Maximum Junction Temperature (T_J) -- +150°C
- Storage Temperature (T_{STG}) --- -65°C to +150°C
- Lead Temperature (Soldering, 10sec.) --- +260°C

Note 1：Stresses beyond those listed under "Absolute Maximum Ratings" may cause permanent damage to the device.

Recommended Operating Conditions

- Supply Voltage (V_{DD}) -- +2.6V to +5.5V
- Operation Temperature Range (T_{OPR}) -- -40°C to +85°C

Electrical Characteristics

(V_{DD}=3.6V, EN=V_{DD}, T_A= 25ºC, unless otherwise specified)

Parameter	Symbol	Conditions	Min.	Typ.	Max.	Unit
Operating Input Voltage	V_{DD}		2.6		5.5	V
Quiescent Current	I_Q	Active, No Load		3.4		mA
Shutdown Current	I_{SD}	EN=GND			1	µA
EN High-Level Input Voltage	V_{IH}		1.4			V
EN Low-Level Input Voltage	V_{IL}				0.4	V
EN Input Leakage Current	I_{LKG}	EN=GND or VDD		0.01		µA
N-Channel MOSFET On-Resistance (Note2)	$R_{DS(ON)}$	I_{LX} = 100mA		95	160	mΩ
P-Channel MOSFET On-Resistance (Note2)	$R_{DS(ON)}$	I_{LX} = 100mA		140	210	mΩ
Oscillator Frequency	fs		0.75	1	1.25	MHz
P-Channel Current Limit (Note2)	I_{LIM}		2.2	3		A
Under Voltage Lock Out Voltage	UVLO			2.43		V
UVLO Hysteresis	V_{HYS}			0.15		V
FB Input Leakage Current	I_{FB}	V_{FB}= V_{DD}		50		nA
LX Leakage Current		V_{DD}=3.6V, V_{LX}=0V or V_{LX}=3.6V		1		µA
Reference Voltage	V_{REF}		0.582	0.6	0.618	V
Line Regulation	ΔV_{LINE}	V_{DD} =V_O+0.5V to 5.5V; I_O = 10mA		0.05		%/V
Load Regulation	ΔV_{LOAD}	I_O = 0A to 2A		0.15		%/A
Thermal Shutdown Temperature (Note2)	T_{SD}			160		°C
	ΔT_{SD}	Hysteresis		20		°C

Note 2：Guarantee by design.

Typical Performance Curves

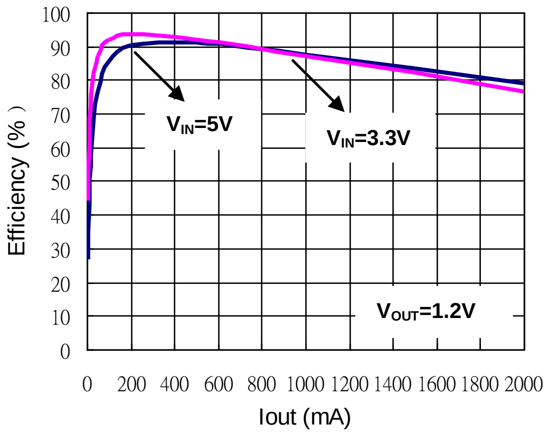


Figure 4. Efficiency vs. Output Current

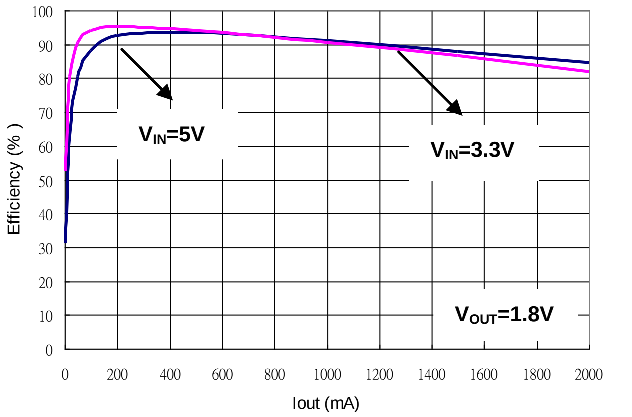


Figure 5.Efficiency vs. Output Current

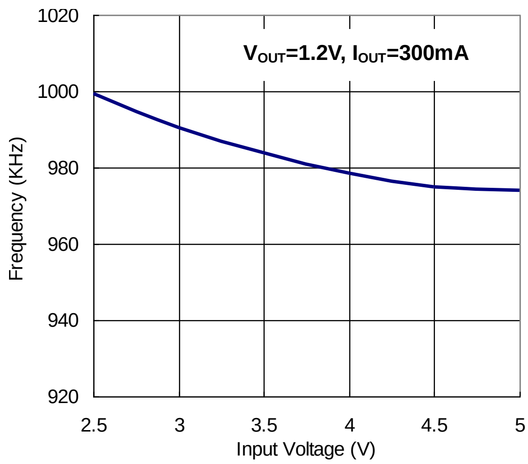


Figure 6. Frequency vs. Input Voltage

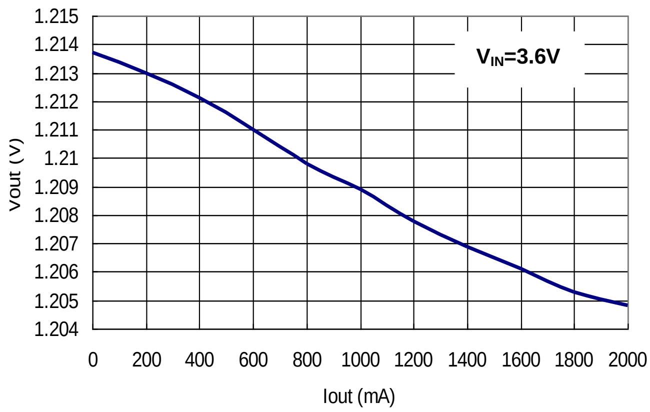


Figure 7. Output Voltage vs. Output Current

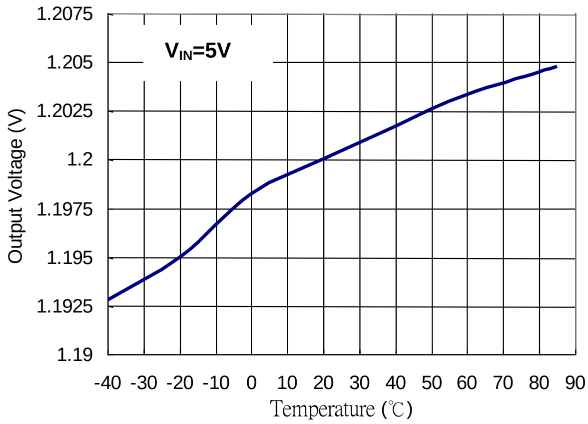


Figure 8. Output Voltage vs. Temperature

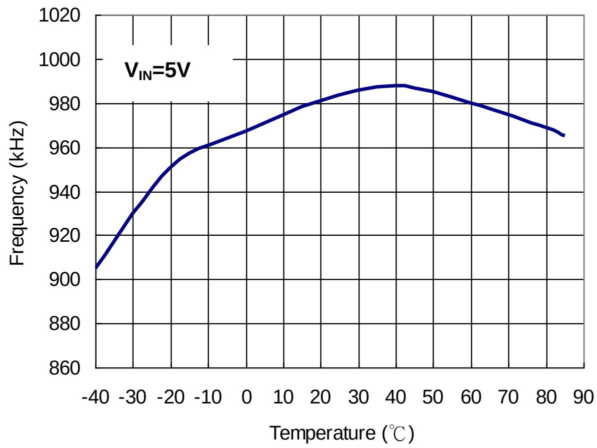


Figure 9. Frequency vs. Temperature

Typical Performance Curves (Continued)

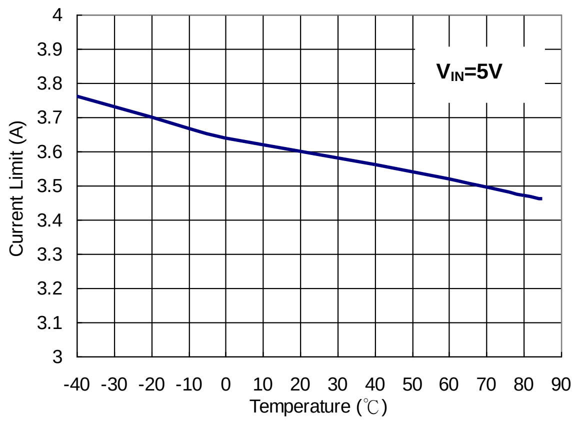


Figure10. Current Limit vs. Temperature

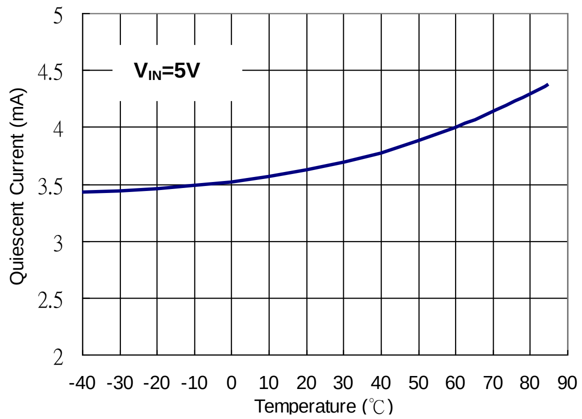


Figure11. Quiescent Current vs. Temperature

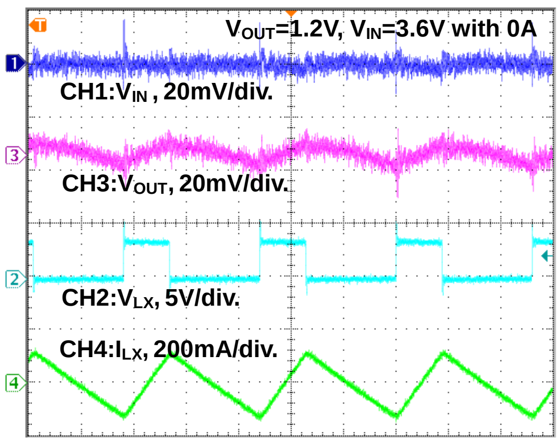


Figure12. Output ripple noise

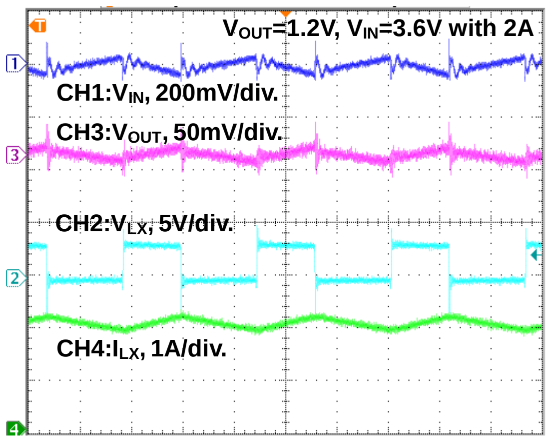


Figure13. Output ripple noise

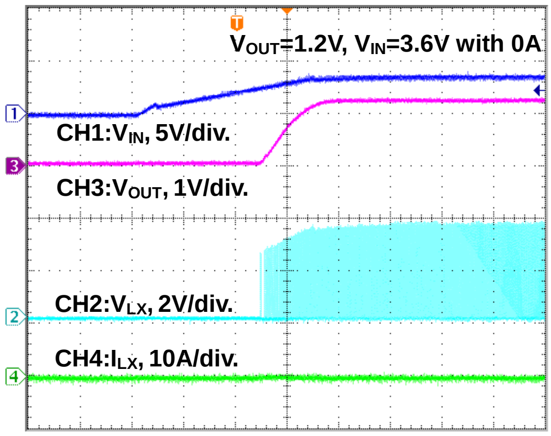


Figure14. Power on form V_{IN}

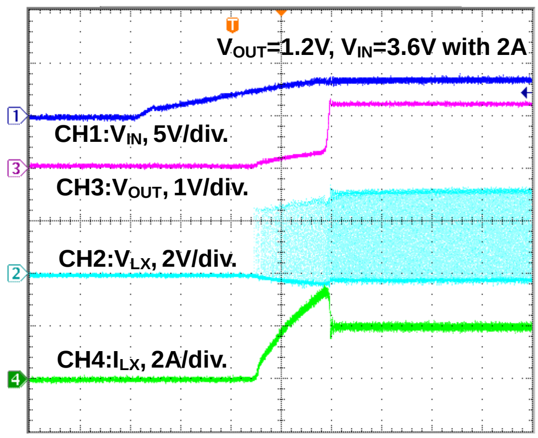


Figure 15. Power on form V_{IN}

Typical Performance Curves (Continued)

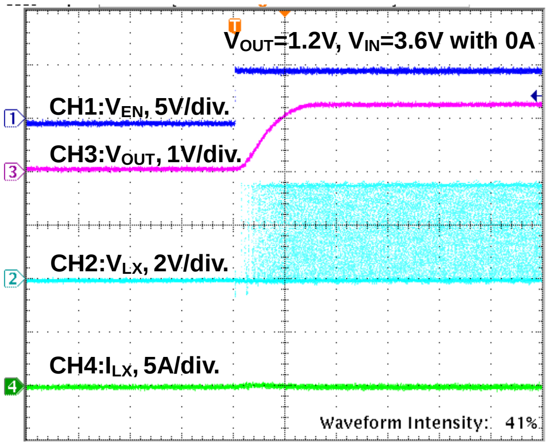


Figure 16. Power on form V_{EN}

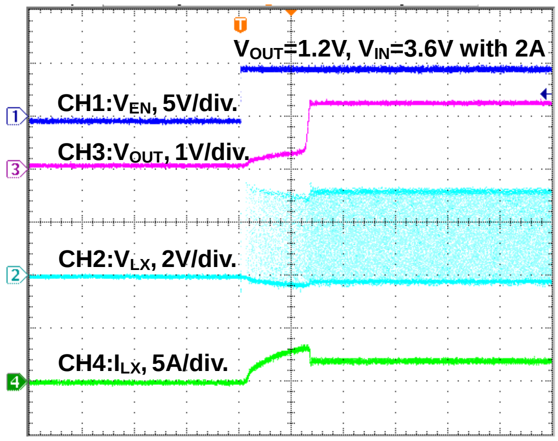


Figure17. Power on form V_{EN}

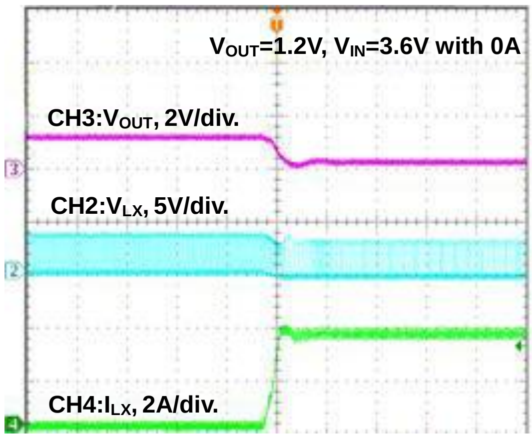


Figure18. Short circuit protection

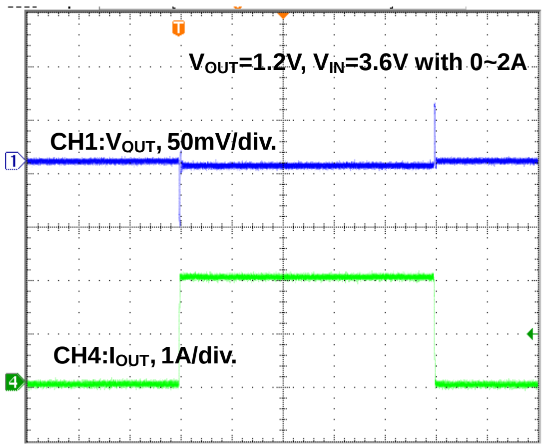


Figure19. Load transient response

Application Information

Inductor Selection

A 2.2μH to 4.7μH is recommended for general used. The value of inductor depends on the operating frequency. Higher frequency allows smaller inductor and capacitor but increases internal switching loss. Two inductor parameters should be considered, current rating and DCR. The inductor with the lowest DCR is chosen for the highest efficiency.

The inductor value can be calculated as:

$$L \geq \frac{V_{OUT}}{f \times \Delta I_L}\left(1-\frac{V_{OUT}}{V_{IN}}\right)$$

ΔI_L: inductor ripple current, which is defined as:

$$\Delta I_L = V_O[(1-\frac{V_O}{V_I})/(L*f)] \quad \text{(General Setting)}$$

$$\approx 0.1*2*I_{O-MAX}$$

The inductor should be rated for the maximum output current ($I_{O\text{-}MAX}$) plus the inductor ripple current (ΔI_L) to avoid saturation. The maximum inductor current ($I_{L\text{-}MAX}$) is given by:

$$I_{L\text{-}MAX} = I_{O\text{-}MAX} + \frac{\Delta I_L}{2}$$

Capacitor Selection

The small size of ceramic capacitors are ideal for FP6361 applications. X5R and X7R types are recommended because they retain their capacitance over wider voltage and temperature ranges than other types, such as Y5V or Z5U. A 10μF input capacitor and two 22μF output capacitors are sufficient for most FP6361 applications.

When selecting an output capacitor, consider the output ripple voltage and the ripple current. The ESR of capacitor is a major factor to the output ripple. For the best performance, a low ESR output capacitor is required. The ripple voltage is given by:

$$\Delta V_O = \Delta I_L\left(ESR + \frac{1}{8 \times f \times C_O}\right)$$

Output Voltage Programming (adjustable voltage version)

The output voltage of FP6361 is set by the resistor divider according to the following formula:

$$V_{OUT} = V_{FB} \times \left(1+\frac{R1}{R2}\right)$$

R1 is the upper resistor of the voltage divider. For transient response reasons, a small feed-forward capacitor (C_F) is required in parallel to the upper feedback resistor, and 33pF is recommended.

Checking Transient Response

The regulator loop response can be checked by looking at the load transient response. Switching regulators take several cycles to respond to a step in load current. When a load step occurs, V_{OUT} will be shifted immediately by an amount equal to (ΔI_{LOAD} • ESR), where ESR is the effective series resistance of C_{OUT}. ΔI_{LOAD} will also begin to charge or discharge C_{OUT}, which generates a feedback error signal. Then the regulator loop will act to return V_{OUT} to its steady state value. During this recovery time, V_{OUT} can be monitored for overshoot or ringing that will indicate the stability problem.

The discharged bypass capacitors are effectively put in parallel with C_{OUT}, causing a rapidly drop in V_{OUT}. No regulator can deliver enough current to prevent this problem if the load switch resistance is low and it is driven quickly. The only solution is to limit the rise time of the switch drive so that the load rise time will be limited to approximately (25 • C_{LOAD}).

Current Mode PWM Control

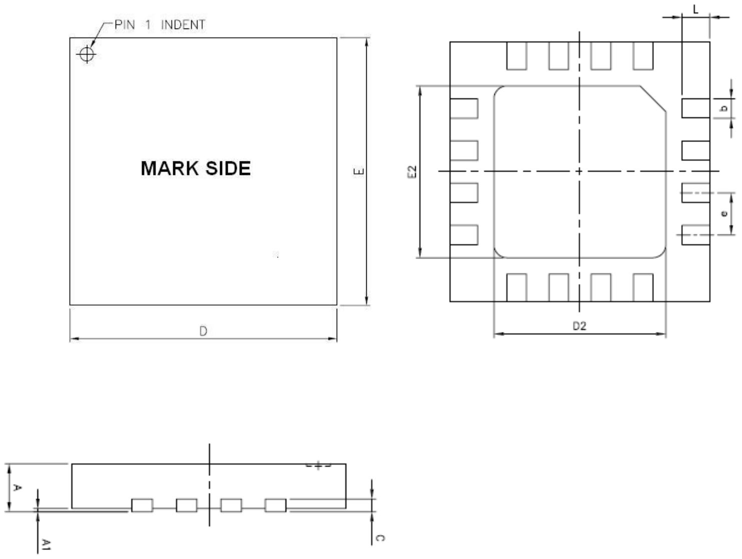
Slope compensated current mode PWM control provides stable switching, cycle-by-cycle current limit for superior load, line response, protection of the internal main switch and synchronous rectifier. The FP6361 switches at a constant frequency (1MHz) and regulates the output voltage. During each cycle, the PWM comparator modulates the power transferred to the load by changing the inductor peak current based on the feedback error voltage. During normal operation, the main switch is turned on for a certain time to ramp the inductor current at each rising edge of the internal oscillator, and switched off when the peak inductor current is above the error voltage. When the main switch is off, the synchronous rectifier will be turned on immediately and stay on until next cycle starts.

Dropout Operation

The FP6361 allows the main switch to remain on for more than one switching cycle, and increases the duty cycle while the input voltage is dropping close to the output voltage. When the duty cycle reaches 100%, the main switch will be held on continuously to deliver current to the output up to the MOSFET current limit. Then the output voltage will be the input voltage minus the voltage drop across the main switch and the inductor.

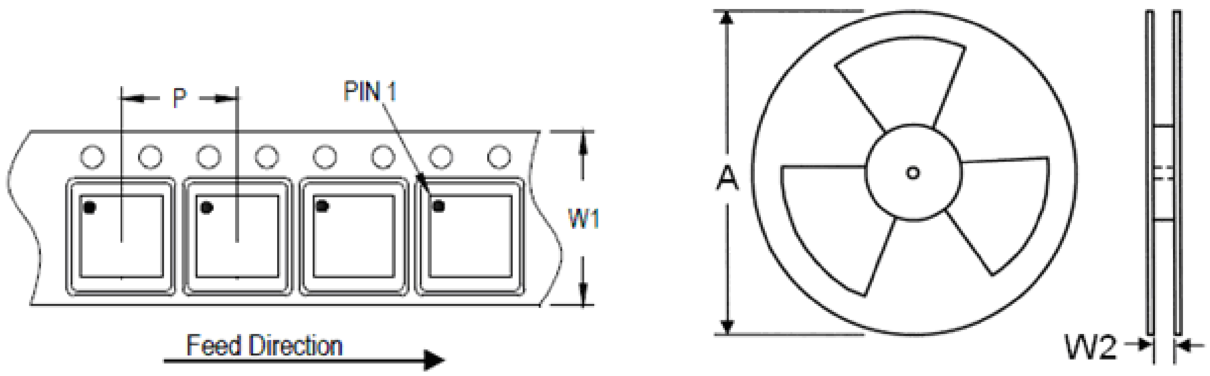
Outline Information

TQFN-16 3mm×3mm Package (Unit: mm)



SYMBOLS UNIT	DIMENSION IN MILLIMETER	
	MIN	MAX
A	0.70	0.80
A1	0.00	0.05
C	0.19	0.30
E	2.90	3.10
D	2.90	3.10
L	0.35	0.45
b	0.18	0.30
e	0.45	0.55
E2	1.50	1.80
D2	1.50	1.80

Carrier Dimensions



Tape Size (W1) mm	Pocket Pitch (P) mm	Reel Size (A)		Reel Width (W2) mm	Empty Cavity Length mm	Units per Reel
		in	mm			
12	8	13	330	12.4	400~1000	3,000

Life Support Policy
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